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(54) Title: DIGITAL AUDIO AMPLIFIER INCLUDING PHASE LEAD-LAG COMPENSATOR FOR INCREASING SELF-OS-
CILLATION FREQUENCY
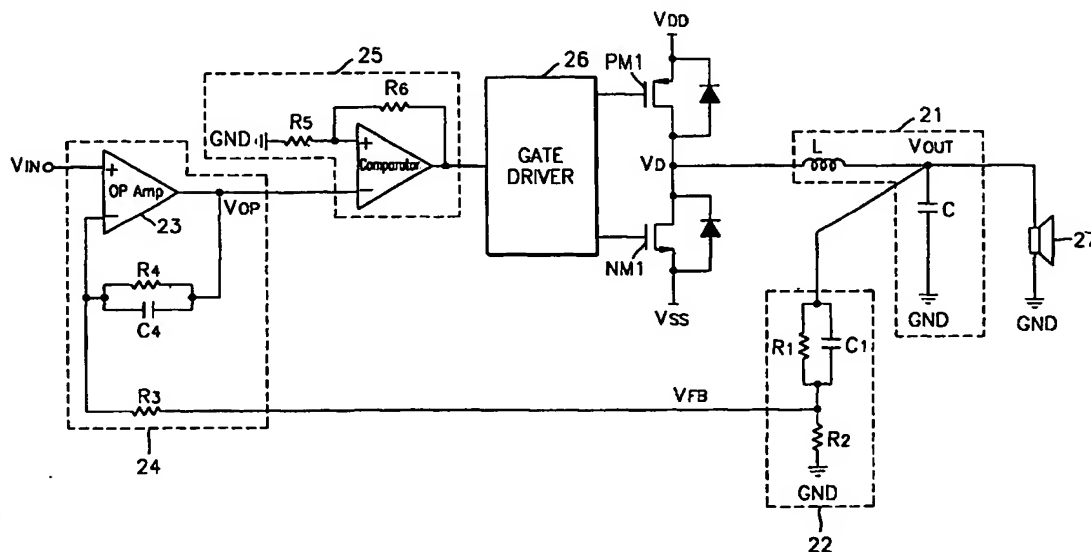
(57) Abstract: Provided is a digital audio amplifier capable of increasing self-oscillation frequency by using a phase lead-lag com-
pensator. The digital audio amplifier includes the phase lead-lag compensator which increases the self-oscillation frequency by
lead-lag-compensating for the phase of an output signal and making a feedback of the compensated output signal. In addition, the
digital audio amplifier further includes a bandwidth control means which controls the bandwidth of an error amplifier. Accordingly,
the digital audio amplifier can adjust the self-oscillation frequency and reduce the extent to which the self-oscillation frequency varies
in accordance with the variation of the output signal by using the bandwidth control means that inserts a pole into the error amplifier.

DIGITAL AUDIO AMPLIFIER INCLUDING PHASE LEAD-LAG COMPENSATOR FOR INCREASING SELF-OSCILLATION FREQUENCY

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Technical Field

The present invention relates to a self oscillation-type digital audio amplifier, and more particularly, to a digital audio amplifier capable of increasing self-oscillation frequency by using a phase lead-lag
10 compensator.

Background Art

FIG. 1 is a circuit diagram of a conventional self oscillation-type digital audio amplifier. Referring to FIG. 1, the conventional self
15 oscillation-type digital audio amplifier includes a power PMOS transistor (PM), a power NMOS transistor (NM), a first filter 11, a second filter 12, a voltage divider 13, an error amplifier 14, a comparator 15, and a gate driver 16.

The operation of the conventional self oscillation-type digital audio
20 amplifier of FIG. 1 will be described in the following paragraphs.

An output voltage V_{OUT} is divided by the voltage divider 13 at a constant rate, and a result of the division, i.e., a feedback voltage V_{FB}, is compared with an input audio voltage V_{IN} by the error amplifier 14. Error amplified by the error amplifier 14 is converted into a pulse signal
25 by the comparator 15 having hysteresis. The pulse signal is transmitted to the power transistors PM and NM via the gate driver 16 and then is finally used for controlling the output voltage V_{OUT}.

More specifically, if the input audio voltage V_{IN} is larger than the feedback voltage V_{FB}, the PMOS transistor PM is turned on so that the
30 output voltage V_{OUT} increases. If the output voltage V_{OUT} keeps increasing until the feedback V_{FB} becomes larger than the input audio

voltage V_{IN}, the NMOS transistor NM is turned on so that the output voltage V_{OUT} decreases.

The conventional self oscillation-type digital audio amplifier operates in an oscillation manner where the output voltage V_{OUT} 5   alternately increases and decreases at high speed centering around a result of amplifying the input voltage V_{IN} at a predetermined rate. The output voltage V_{OUT} has a waveform obtained by adding a voltage ripple generated in self-oscillation to a result of amplifying the input signal VIN having a voice bandwidth of 20 Hz ~ 20 kHz at a predetermined rate. 10   Here, the voltage ripple is a voltage component having an amplitude of about 100 mV and having a higher frequency than voice signals. In the meantime, since the power switches, i.e., the power transistors PM and NM, automatically operate while the conventional self oscillation-type digital   audio   amplifier   undergoes   self-oscillation,   self-oscillation 15   frequency can be simply called switching frequency.

In the conventional self oscillation-type digital audio amplifier of FIG. 1, a resistor R_1 and a capacitor C_1 in the first filter 11 are connected to each other in cascade in order to sense the variation of the output voltage V_{OUT}.   Accordingly, the variation of voltage at the capacitor C_1 is 20   proportional to the amount of current passing through the capacitor C_1. A difference between voltages respectively at either end of the resistor R_1 corresponds to the variation of the voltage at the capacitor C_1. Therefore, as large a waveform as the variation of the voltage at the capacitor C_1 can be obtained by increasing the resistance of the resistor 25 R_1.

The conventional self oscillation-type digital audio amplifier can feed back the output voltage V_{OUT} and its variation by sensing the variation of the voltage at the capacitor C_1 taking advantage of the above-described structure of the first filter 11 in which the resistor R_1 and 30   the capacitor C_1 are connected to each other in cascade. However, a voltage ripple at the output node (V_{OUT}) of the capacitor C_1 may

undesirably increase. In order to prevent this problem, excessive voltage ripples should be compensated for by connecting the first filter 11 and the second filter 12 in cascade.

Alternatively, voltage ripples at the output node (V_{OUT}) can be
5   sufficiently compensated for by providing the first filter 11 without the resistor R1. In this case, however, self-oscillation frequency may dramatically decrease.

Disclosure of the Invention

10   The present invention provides a self oscillation-type digital audio amplifier which is capable of increasing self-oscillation frequency by lead-lag-compensating for the phase of an output signal and making a feedback of the compensated output signal and is also capable of adjusting the self-oscillation frequency and decreasing the extent to
15   which the self-oscillation frequency varies in accordance with the variation of the output signal by controlling the bandwidth of an error amplifier.

According to an aspect of the present invention, there is provided a digital audio amplifier. The digital audio amplifier includes a power
20   PMOS transistor, which has a source to which a first power supply voltage is applied and a drain connected to a common node, a power NMOS transistor, which has a drain connected to the common node and a source to which a second power supply voltage is applied, an output node filter, which is connected to the common node, a phase lead-lag
25   compensator, which lead-lag compensates for the phase of an output signal of the output node filter, an error amplifier, which compares an output signal of the phase lead-lag compensator with an input audio signal and amplifies an error between the output signal and the input audio signal, a comparator, which converts an error amplified by the error
30   amplifier into a pulse signal, and a gate driver, which controls a gate of the power PMOS transistor and a gate of the power NMOS transistor in

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response to the pulse signal. Here, the phase lead-lag compensator increases self-oscillation frequency by lead-lag-compensating for the phase of the output signal of the output node filter.

Preferably, the digital audio amplifier further includes a bandwidth control means, which adjusts the bandwidth of the error amplifier.

Brief Description of the Drawings

The above and other features and advantages of the present invention will become more apparent by describing in detail exemplary embodiments thereof with reference to the attached drawings in which:

FIG. 1 is a circuit diagram of a conventional self oscillation-type digital audio amplifier;

FIG. 2 is a circuit diagram of a self oscillation-type digital audio amplifier according to a preferred embodiment of the present invention;

FIG. 3 is a diagram illustrating the variation of gain and phase delay in accordance with frequency of a phase lead-lag compensator of FIG. 2;

FIG. 4 is a diagram illustrating limiting of amplification frequency bandwidth by using a bandwidth control means that inserts a pole into an error amplifier of FIG. 2;

FIG. 5 is a diagram illustrating the frequency characteristics of an entire feedback loop in the self oscillation-type digital audio amplifier of FIG. 2;

FIG. 6 is a circuit diagram of a self oscillation-type digital audio amplifier according to a second embodiment of the present invention; and

FIGS. 7 through 9 are circuit diagrams of different examples of the phase lead-lag compensator of FIG. 2 or 6.

Best mode for carrying out the Invention

Hereinafter, the present invention will be described more fully with reference to the accompanying drawings in which preferred embodiments of the invention are shown.

FIG. 2 is a circuit diagram of a self oscillation-type digital audio amplifier according to a preferred embodiment of the present invention. Referring to FIG. 2, the self oscillation-type digital audio amplifier includes a power PMOS transistor PM1, a power NMOS transistor NM1, an output node filter 21, a phase lead-lag compensator 22, an error amplifier 24, a comparator 25, and a gate driver 26. A speaker 27 is connected to the output node filter 21.

A first power supply voltage V_{DD}, i.e., a positive power supply voltage, is applied to the source of the power PMOS transistor PM1, and a common node V_D is connected to the drain of the power PMOS transistor PM1. On the other hand, the common node V_D is connected to the drain of the power NMOS transistor NM1, and a second power supply voltage V_{SS}, i.e., a negative power supply voltage, is applied to the source of the power NMOS transistor NM1.

The output node filter 21 is connected to the common node V_D, and a final output signal V_{OUT} of the self oscillation-type digital audio amplifier is output from the output node filter 21. The output node filter 21 includes an inductor L provided between the common node V_D and an output node V_{OUT} of the output node filter 21 and a capacitor C provided between the output node V_{OUT} of the output node filter 21 and ground voltage GND.

The phase lead-lag compensator 22 lead-lag compensates the phase of the output signal V_{OUT} received from the output node filter 21 and then outputs a result of the lead-lag compensation. The phase lead-lag compensator 22 includes a first resistor R_1 provided between the output node of the output node filter 21 and the output node of the phase lead-lag compensator 22, a capacitor C_1 connected to the first resistor R_1 in parallel, and a second resistor R_2 provided between the an

output node of the phase lead-lag compensator 22 and the ground voltage GND.

The error amplifier 24 compares an output signal V_{FB} of the phase lead-lag compensator 22 with an input audio signal V_{IN} and amplifies an error between the output signal V_{FB} and the input audio signal V_{IN}. The comparator 25 converts the amplified error received from the error amplifier 24 into a pulse signal, and the gate driver 26 controls the gate of the power PMOS transistor PM1 and the gate of the power NMOS transistor NM1 in response to the pulse signal.

The error amplifier 24 includes an operational amplifier whose output node is connected to an input node of the comparator 25 and whose first input node is connected to the input audio signal V_{IN}, a third resistor R_3 provided between an output node V_{FB} of the phase lead-lag compensator 22 and a second input node of the operational amplifier 23, a fourth resistor R_4 provided between the second input node of the operational amplifier 23 and an output node V_{OP}, and a capacitor C_4 connected to the fourth resistor R_4 in parallel. Functions of the error amplifier 24 whose bandwidth is limited are determined by the capacitor C_4. In other words, a pole is generated at a predetermined frequency at which the capacitor C_4 and the fourth resistor R_4 have the same impedance.

Hereinafter, the operation of the self oscillation-type digital audio amplifier according to the present invention, shown in FIG. 2, will be described in greater detail. In principle, an oscillator oscillates at a predetermined frequency that provides a phase delay of a total of 360 degrees and a gain of 1 or larger in an entire feedback loop. The self-oscillation frequency can be increased by increasing the phase margin of the feedback loop. From a phase's point of view, the conventional self oscillation-type digital audio amplifier of FIG. 1 increases its phase margin by inserting the cascade resistor R_1 into the capacitor C_1, while the self oscillation-type digital audio amplifier

according to the present invention increases its phase margin by using the phase lead-lag compensator 22.

FIG. 3 is a diagram illustrating the variation of gain and phase delay depending on frequency of the phase lead-lag compensator 22 of FIG. 2. The phase lead-lag compensator 22 can compensate for phase delay generated at the output node filter 21. According to the frequency characteristics of the phase lead-lag compensator 22, a zero point is created by the first resistor R_1 and the capacitor C_1, and gain increases. If the frequency of the phase lead-lag compensator 22 increases during a phase lead, the gain stops increasing due to a pole created by the capacitor C_1 and the first and second resistors R_1 and R_2 connected to each other in parallel, and the phase lead decreases. Then, the original phase is recovered at a frequency 10 times higher than the pole.

Therefore, phase margin can be generated at frequencies between the zero point and the pole by leading the output node filter 21. The phase margin indicates that phase delay caused by the error amplifier 24 and the comparator 25 may possibly increase. The phase margin increases self-oscillation frequency.

FIG. 4 is a diagram illustrating limiting of amplification frequency bandwidth by using the bandwidth control means C_4 that inserts a pole into the error amplifier 24. The error amplifier 24 into which a pole is inserted maintain uniform gain at frequencies lower than the pole but has decreasing gain and lengthened phase delay at frequencies higher than the pole. If the pole moves within the phase variation bandwidth of the phase lead-lag compensator 22, phase delay of the entire feedback loop varies at self-oscillation frequency or so, and accordingly, the self-oscillation frequency itself varies. The error amplifier 24 into which the pole is inserted may possibly be seen as an amplifier whose operation bandwidth is limited.

FIG. 5 is a diagram illustrating the frequency characteristics of an entire feedback loop in a self oscillation-type digital audio amplifier

according to a preferred embodiment of the present invention. A low pass filter, i.e., the output node filter 21 of FIG. 2, which is an secondary inductor-capacitor filter, removes self-oscillation frequency components whose frequency is higher than that of the input audio signal V_{IN} from a signal output from the common node VD of the power MOS transistors PM1 and NM1. In the output node filter 21, the gain of a voltage component whose frequency is higher than self-oscillation frequency (f) decreases to 40 dB/dec, and the phase of the voltage component is delayed by as much as 180 degrees. Here, $f = \dfrac{1}{2\pi\sqrt{LC}} \cong 20kHz$.

However, if the frequency of the voltage component further increases, a zero point is created due to parasitic resistance existing in the capacitor C, and a phase lead occurs. Since it is generally generated at a frequency of several MHz or higher, the zero point is almost ignored.

The output signal V_{OUT} of the output node filter 21 is converted into the feedback signal V_{FB} after its amplitude is decreased and its phase is led by the phase lead-lag compensator 22. The error amplifier 24 compares the feedback signal V_{FB} with the input audio signal V_{IN}, input from the outside of the self oscillation-type digital audio amplifier of FIG. 2, and amplifies a difference between the feedback signal V_{FB} and the input audio signal V_{IN}.

While signals travel along the feedback loop in the self oscillation-type digital audio amplifier of FIG. 2, phase delay additionally occurs in the comparator 25 and the gate driver 26. In the power MOS transistors PM1 and NM1, in particular, phase inversion occurs, and accordingly, a phase delay of 180 degrees occurs. Finally, the self oscillation-type digital audio amplifier of FIG. 2 starts oscillating at a predetermined frequency where a total phase delay of 360 degrees can be obtained with a loop gain of 1 or larger. Gain and phase delay can be adjusted by using the phase lead-lag compensator 22 and the error amplifier. If a self oscillation-type digital audio amplifier includes the

output node filter 21 without the phase lead-lag compensator 22, self-oscillation frequency remains at several tens of kHz. On the other hand, if the self oscillation-type digital audio amplifier, like the one shown in FIG. 2, includes the phase lead-lag compensator 22 as well as the output node filter 21, the self-oscillation frequency increases to several hundreds of kHz.

In FIGS. 3 through 5, frequency (W) and gain (Gain) are represented using a log scale.

In a self oscillation-type digital audio amplifier, self-oscillation frequency decreases as output voltage increases. If bandwidth is limited by inserting a pole into the error amplifier 24 using the bandwidth control means C_4, the extent to which the self-oscillation frequency varies in accordance with the variation of the output voltage can be reduced. In other words, if the self-oscillation frequency decreases, the error amplifier 24 increases gain and decreases phase delay. On the other hand, if the self-oscillation frequency increases, the error amplifier 24 decreases the gain and increases the phase delay. By dong so, the error amplifier 24 can prevent fluctuations in the self-oscillation frequency in accordance with the variation of the output voltage.

FIG. 6 is a circuit diagram of a self oscillation-type digital audio amplifier according to another preferred embodiment of the present invention. Referring to FIG. 6, the self oscillation-type digital audio amplifier, like the self oscillation-type digital audio amplifier of FIG. 2, includes a power PMOS transistor PM1, a power NMOS transistor NM1, a phase lead-lag compensator 22, an error amplifier 24, a comparator 25, a gate driver 26, and a speaker 27. In addition, the self oscillation-type digital audio amplifier further includes an output node filter 61 in which, unlike in the output node filter 21 of FIG. 2, a resistor R is provided between a capacitor C and ground voltage GND.

In the present embodiment, self-oscillation frequency of an entire feedback loop increases due to the existence of the resistor R in the

output node filter 61.   More specifically, due to the resistor R connected to the capacitor C in cascade, a zero point created due to parasitic resistance ESR and the capacitor C moves down so that phase delay occurring in the output node filter 61 decreases and phase margins in the

5.   error amplifier 24, the comparator 25, and the gate driver 26 increase. Accordingly, the self oscillation-type digital audio amplifier can oscillate at higher frequency.

FIGS. 7 through 9 are diagrams illustrating different examples of the phase lead-lag compensator 22 of FIG. 2 or 6.

10   Referring to FIG. 7, a phase lead-lag compensator includes a resistor R_1 provided between an output node V_{OUT} of an output node filter and an inner node N, a capacitor C_1 connected to the resistor R_1 in parallel between the output node V_{OUT} and the inner node N, a resistor R_2 provided between an output node V_{FB} of the phase lead-lag

15   compensator and the inner node N, and a resistor R_3 provided between the output node V_{FB} of the phase lead-lag compensator and ground voltage GND.

Referring to FIG. 8, a phase lead-lag compensator includes a resistor R_1 provided between an output node V_{OUT} of an output node filter

20   and an output node V_{FB} of the phase lead-lag compensator, a resistor R_2 provided between the output node V_{FB} of the phase lead-lag compensator and an inner node N, a resistor R_3 provided between the inner node N and ground voltage GND, and a capacitor C_1 provided between the output node V_{OUT} of the output node filter and the inner

25   node N.

Referring to FIG. 9, a phase lead-lag compensator includes a resistor R_1 provided between an output node V_{OUT} of an output node filter 62 and an output node V_{FB} of the phase lead-lag compensator, a capacitor C_1 connected to the resistor R_1 in parallel between the output

30   node V_{OUT} of the output node filter 62 and the output node V_{FB} of the phase lead-lag compensator, a resistor R_2 provided between the output

node V_{FB} of the phase lead-lag compensator and ground voltage GND, and a capacitor C_b provided between the output node V_{FB} of the phase lead-lag compensator and a connection node N between a capacitor C and a resistor R in the output node filter 62.

5   While the present invention has been particularly shown and described with reference to exemplary embodiments thereof, it will be understood by those of ordinary skill in the art that various changes in form and details may be made therein without departing from the spirit and scope of the present invention as defined by the following claims.

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Industrial Applicability

As described above, the self oscillation-type digital audio amplifier according to the present invention is capable of increasing self-oscillation frequency by lead-lag-compensating for the phase of an output signal

15   and making a feedback of the compensated output signal, and is also capable of adjusting the self-oscillation frequency and reducing the extent to which the self-oscillation frequency varies in accordance with the variation of the output signal by controlling the bandwidth of an error amplifier, i.e., by inserting a pole into the error amplifier.

What is claimed is:

1. A digital audio amplifier comprising:

a power PMOS transistor which has a source to which a first power supply voltage is applied and a drain connected to a common node;

a power NMOS transistor which has a drain connected to the common node and a source to which a second power supply voltage is applied;

an output node filter which is connected to the common node;

a phase lead-lag compensator which lead-lag compensates for the phase of an output signal of the output node filter;

an error amplifier which compares an output signal of the phase lead-lag compensator with an input audio signal and amplifies an error between the output signal and the input audio signal;

a comparator which converts an error amplified by the error amplifier into a pulse signal; and

a gate driver which controls a gate of the power PMOS transistor and a gate of the power NMOS transistor in response to the pulse signal,

wherein the phase lead-lag compensator increases self-oscillation frequency by lead-lag-compensating for the phase of the output signal of the output node filter.

2. The digital audio amplifier of claim 1 further comprising a bandwidth control means which adjusts the bandwidth of the error amplifier.

3. The digital audio amplifier of claim 1, wherein the phase lead-lag compensator comprises:

a first resistor which is provided between an output node of the output node filter and an output node of the phase lead-lag compensator;

a capacitor which is connected to the first resistor in parallel

between the output node of the output node filter and the output node of the phase lead-lag compensator; and

a second resistor which is provided between the output node of the phase lead-lag compensator and ground voltage.

4. The digital audio amplifier of claim 1, wherein the phase lead-lag compensator comprises:

a first resistor which is provided between an output node of the output node filter and an inner node;

a capacitor which is connected to the first resistor in parallel between the output node of the output node filter and the inner node;

a second resistor which is provided between the inner node and an output node of the phase lead-lag compensator; and

a third resistor which is provided between the output node of the phase lead-lag compensator and ground voltage.

5. The digital audio amplifier of claim 1, wherein the phase lead-lag compensator comprises:

a first resistor which is provided between an output node of the output node filter and an output node of the phase lead-lag compensator;

a second resistor which is provided between the output node of the phase lead-lag compensator and an inner node;

a third resistor which is provided between the inner node and ground voltage; and

a capacitor which is provided between the output node of the output node filter and the inner node.

6. The digital audio amplifier of claim 2, wherein the error amplifier comprises:

an operational amplifier which has an output node connected to an input node of the comparator and a first input node connected to the

input audio signal;

a first resistor which is provided between an output node of the phase lead-lag compensator and a second input node of the operational amplifier;

5   a second resistor which is provided between the second input node of the operational amplifier and the output node of the operational amplifier; and

a capacitor which is connected to the second resistor in parallel between the second input node and output node of the operational

10   amplifier.

7.   The digital audio amplifier of claim 1, wherein the output node filter comprises:

an inductor which is provided between the common node and an

15   output node of the output node filter;

a first capacitor one end of which is connected to the output node of the output node filter; and

a first resistor which is provided between the other end of the first capacitor and ground voltage.

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8.   The digital audio amplifier of claim 7, wherein the phase lead-lag compensator comprises:

a second resistor which is provided between the output node of the output node filter and the output node of the phase lead-lag
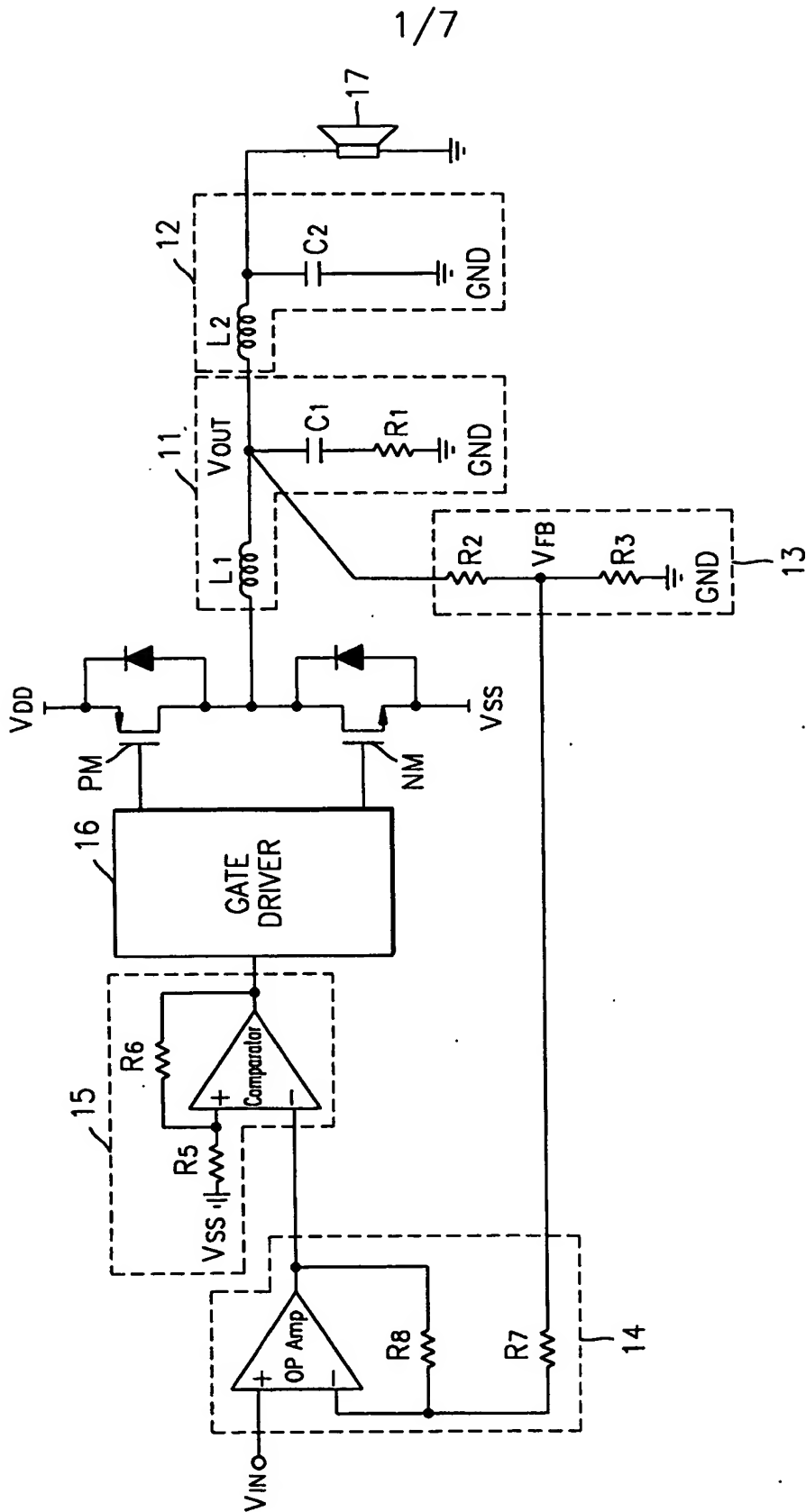
25   compensator;

a second capacitor which is connected to the second resistor in parallel between the output node of the output node filter and the output node of the phase lead-lag compensator;

a third resistor which is provided between the output node of the

30   phase lead-lag compensator and the ground voltage; and

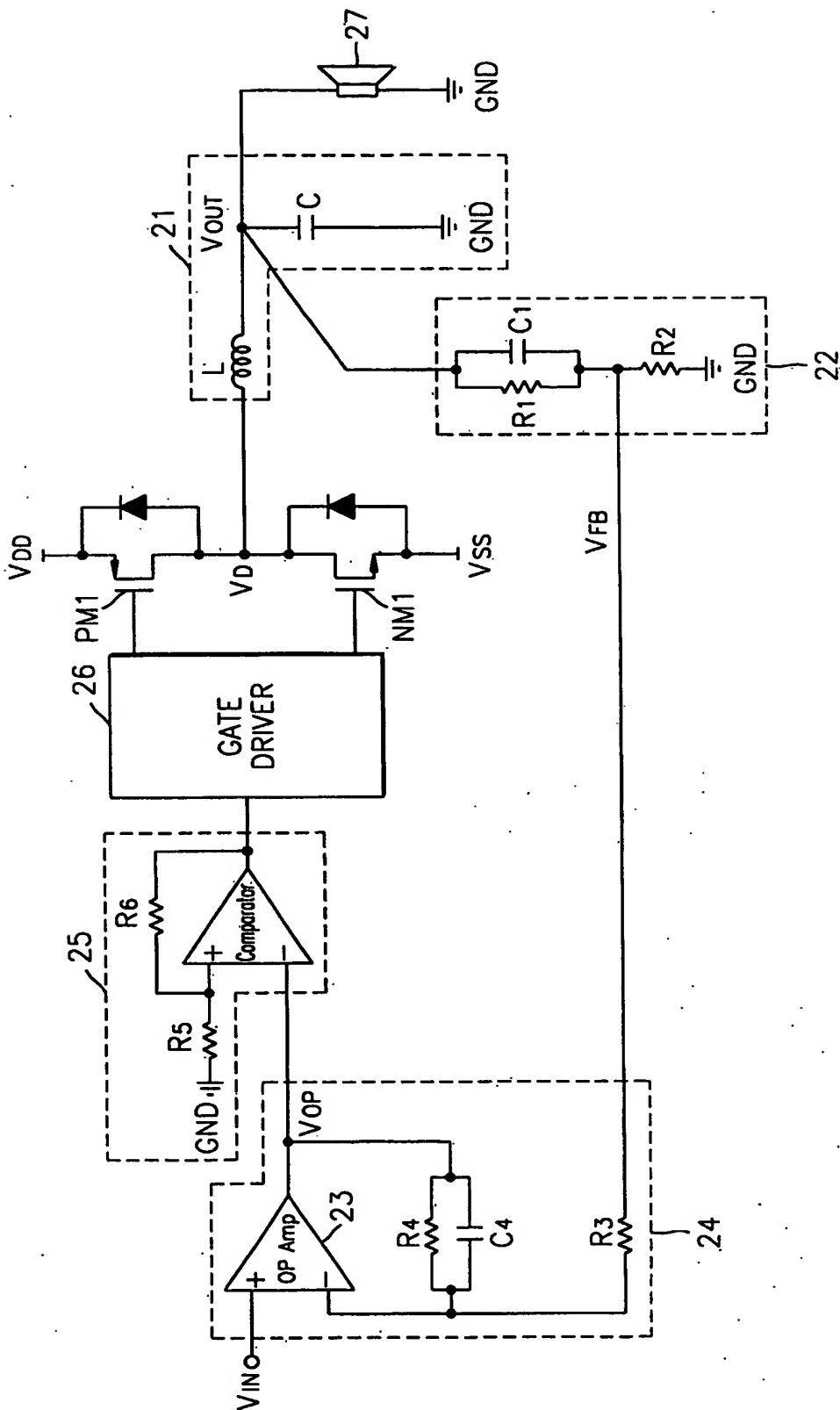a third capacitor which is provided between the output node of the

phase lead-lag compensator and the other end of the first capacitor.
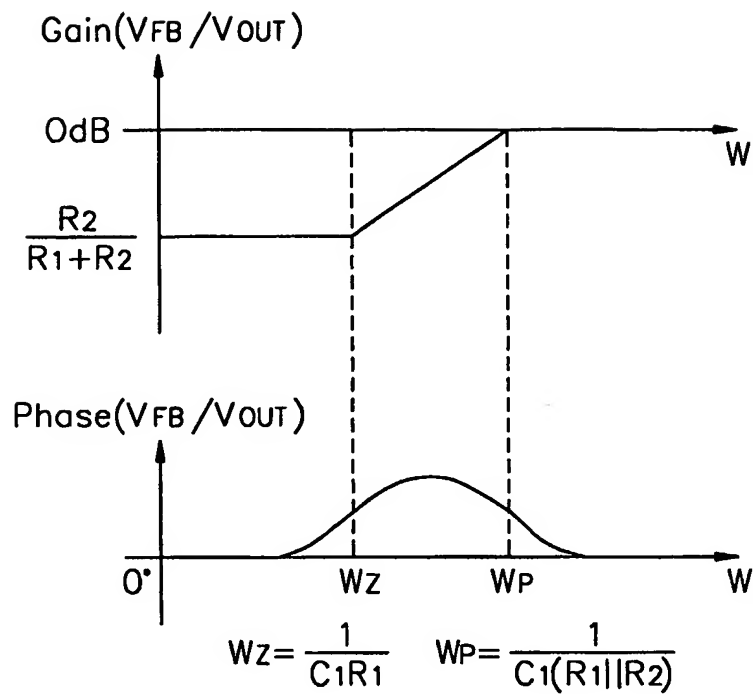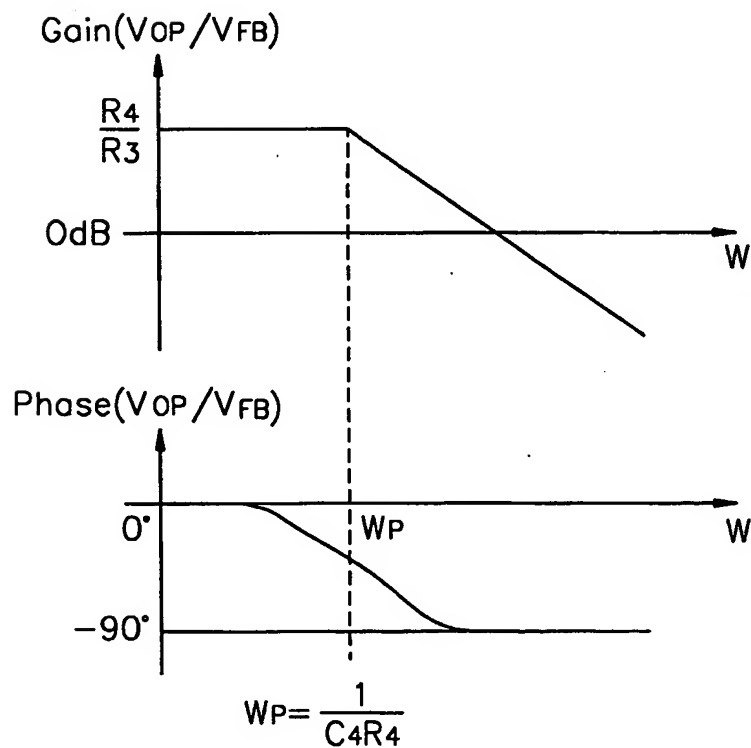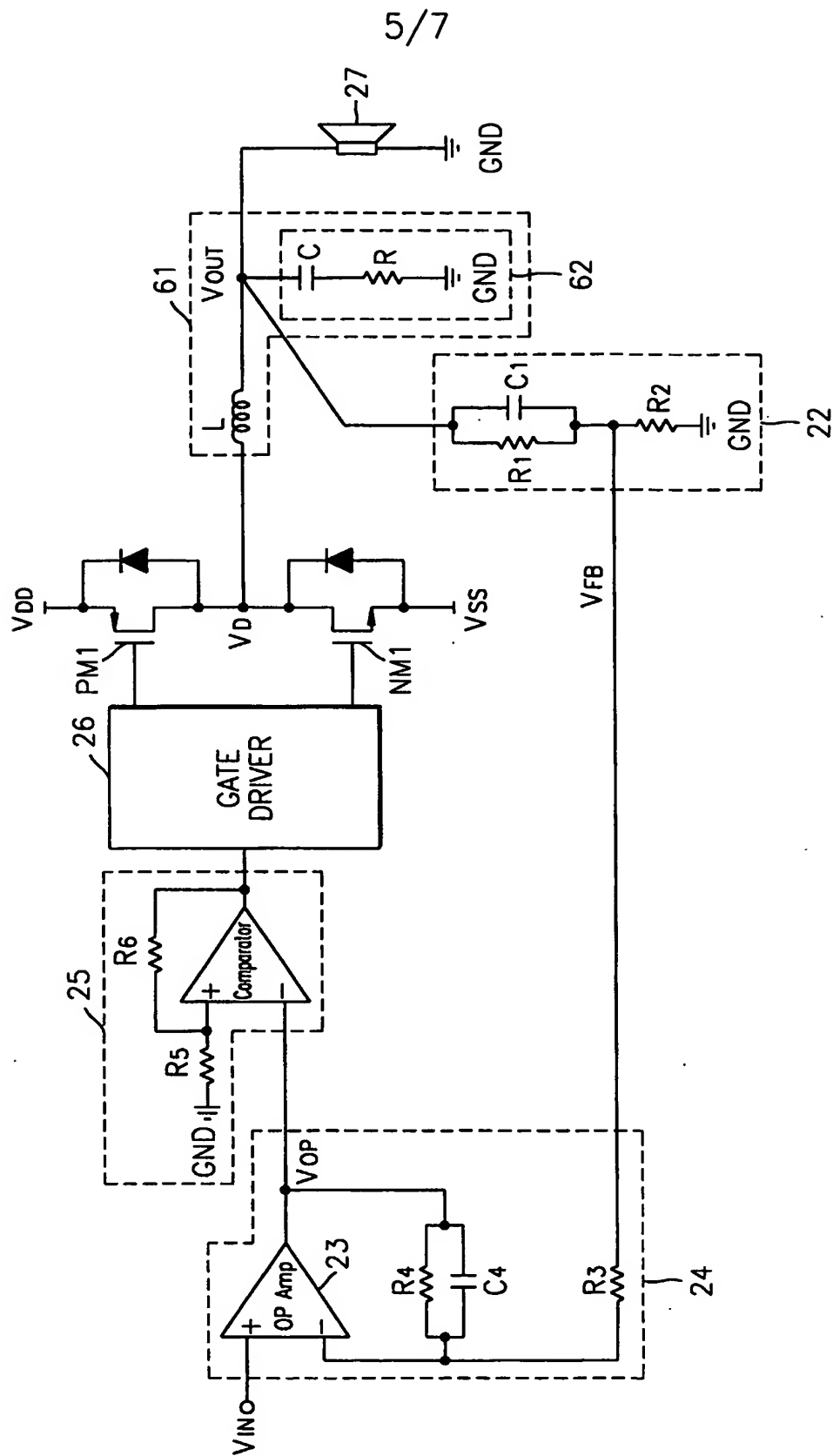
FIG. 1

2/7

FIG. 2
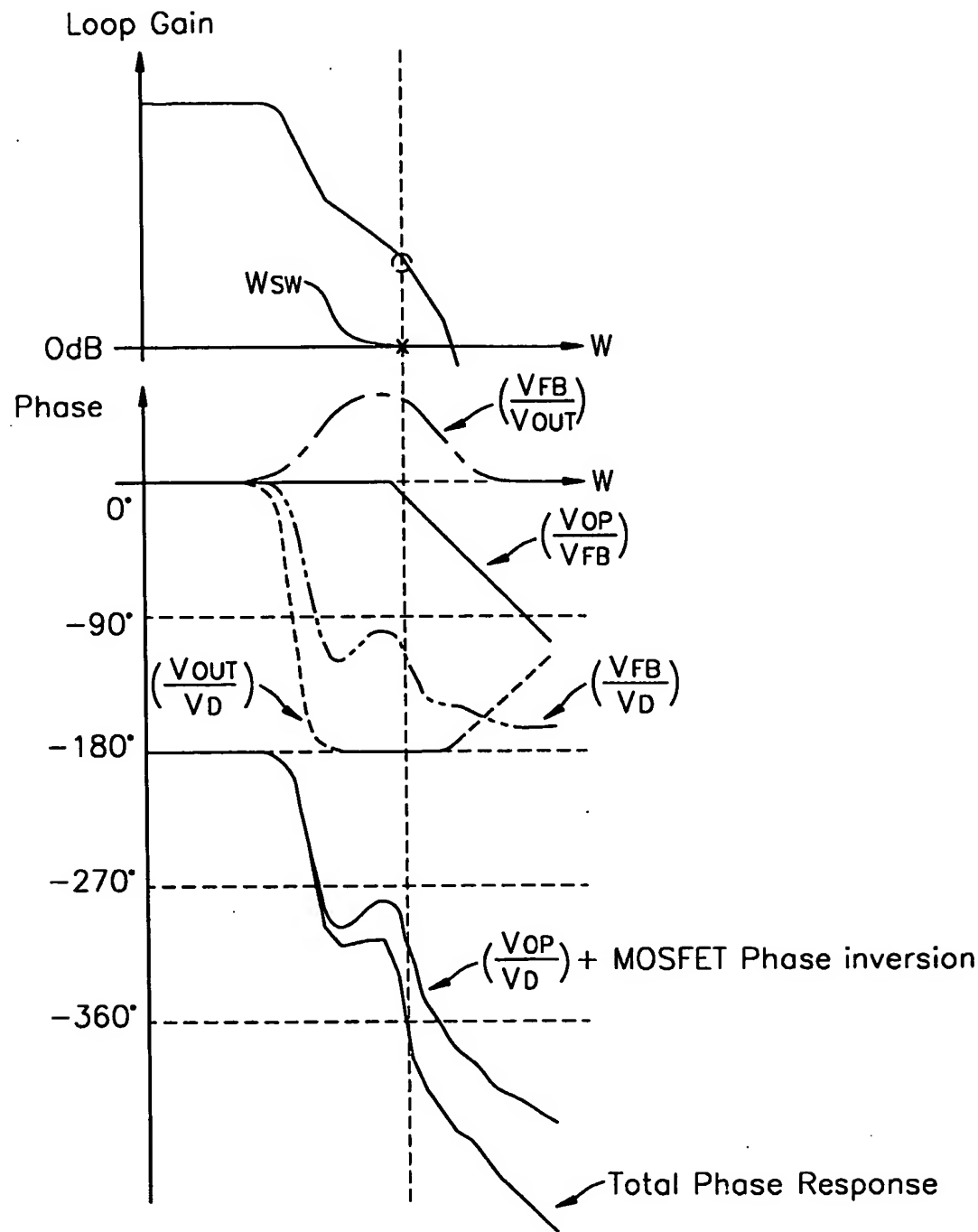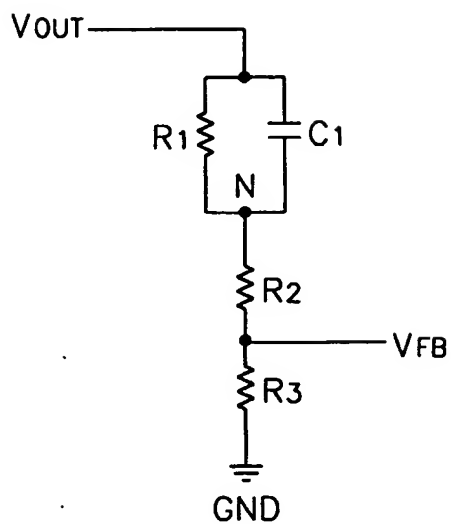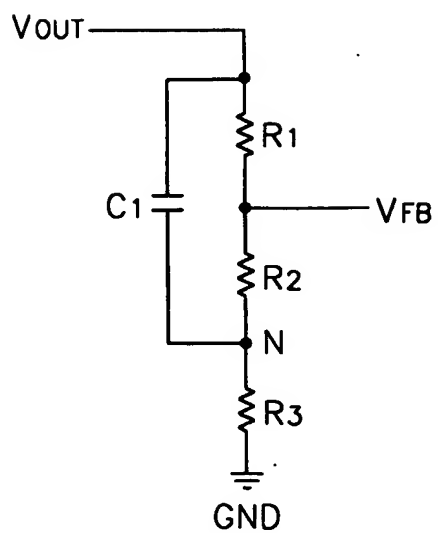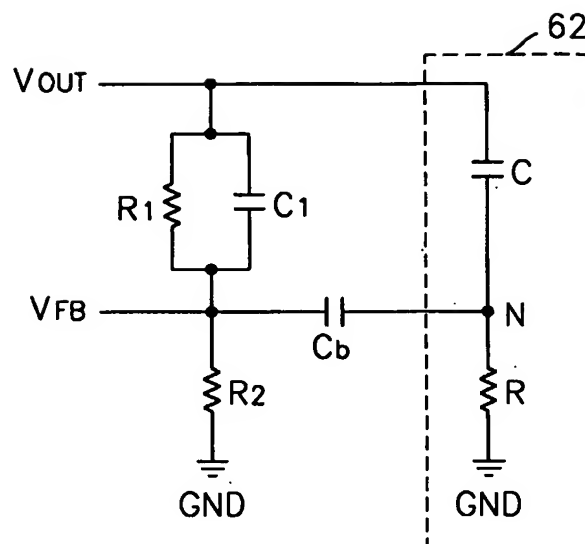
FIG. 3

Gain(V_{FB}/V_{OUT})

OdB

$$\frac{R_2}{R_1+R_2}$$

W

Phase(V_{FB}/V_{OUT})

0° W_Z W_P W

$$W_Z = \frac{1}{C_1 R_1} \qquad W_P = \frac{1}{C_1(R_1 || R_2)}$$

FIG. 4

Gain(V_{OP}/V_{FB})

$$\frac{R_4}{R_3}$$

OdB

W

Phase(V_{OP}/V_{FB})

0° W_P W

−90°

$$W_P = \frac{1}{C_4 R_4}$$

FIG. 5

FIG. 6

FIG. 7

VOUT

R1 C1

N

R2

VFB

R3

GND

FIG. 8

VOUT

C1 R1

VFB

R2

N

R3

GND

FIG. 9

INTERNATIONAL SEARCH REPORT

A. CLASSIFICATION OF SUBJECT MATTER

IPC7 H03G 3/20

According to International Patent Classification (IPC) or to both national classification and IPC

B. FIELDS SEARCHED

Minimum documentation searched (classification system followed by classification symbols)

IPC7 H03G 3/20 H03F 3/217, 3/30, 3/68 H04S 1/00

Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched
  Korean Patents and applications for inventions since 1975
  Korean Utility Models and applications for Utility Models since 1975

Electronic data base consulted during the intertnational search (name of data base and, where practicable, search terms used)
  eKIPAS

C. DOCUMENTS CONSIDERED TO BE RELEVANT

Category*	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
X	US 2002/0097091 A1(Hideto Takagishi) 25 July 2002 see the whole document	1-3, 7-8
Y	US 4464634 A (VSP Labs, Ins.,) 7 August 1984 see the whole document	1-8
A	JP 2000-184500 A (Accuphase Laboratory Inc) 30 Jun 2000 see the whole document	1-8
A	US 5898340 A (Manjimath A. Chatterjee.314-K) 27 April 1999 see the whole document	1-8

☐ Further documents are listed in the continuation of Box C.   ☐ See patent family annex.

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"&" document member of the same patent family

Date of the actual completion of the international search	Date of mailing of the international search report
19 JANUARY 2004 (19.01.2004)	19 JANUARY 2004 (19.01.2004)

Name and mailing address of the ISA/KR	Authorized officer
Korean Intellectual Property Office 920 Dunsan-dong, Seo-gu, Daejeon 302-701, Republic of Korea Facsimile No. 82-42-472-7140	KWON, Ho Young Telephone No. 82-42-481-5676